LM4766 Overture™ Audio Power Amplifier Series Dual 40W Audio Power Amplifier with Mute

General Description
The LM4766 is a stereo audio amplifier capable of delivering typically 40W per channel of continuous average output power into an 8Ω load with less than 0.1% (THD + N).

The performance of the LM4766, utilizing its Self Peak Instantaneous Temperature ('Ke') (SPIKe™) Protection Circuitry, places it in a class above discrete and hybrid amplifiers by providing an inherently, dynamically protected Safe Operating Area (SOA). SPIKe Protection means that these parts are safeguarded at the output against overvoltage, undervoltage, overloads, including thermal runaway and instantaneous temperature peaks.

Each amplifier within the LM4766 has an independent smooth transition fade-in/out mute that minimizes output pops. The IC's extremely low noise floor at 2 µV and its extremely low THD + N value of 0.06% at the rated power make the LM4766 optimum for high-end stereo TVs or mini-component systems.

Key Specifications
- THD+N at 1 kHz at 2 x 30W continuous average output power into 8Ω: 0.1% (max)
- THD+N at 1 kHz at continuous average output power of 2 x 30W into 8Ω: 0.009% (typ)

Features
- SPIKe Protection
- Minimal amount of external components necessary
- Quiet fade-in/out mute mode
- Non-Isolated 15-lead TO-220 package

Applications
- High-end stereo TVs
- Component stereo
- Compact stereo

Typical Application

Figure 1. Typical Audio Amplifier Application Circuit

Note: Numbers in parentheses represent pinout for amplifier B.
*Optional component dependent upon specific design requirements.
Absolute Maximum Ratings (Notes 4, 5)

If Military/Aerospace specified devices are required, please contact the National Semiconductor Sales Office/ Distributors for availability and specifications.

Supply Voltage $|V_{CC}| + |V_{EE}|$
- (No Input) 78V
- (with Input) 74V
Common Mode Input Voltage $(V_{CC}$ or $V_{EE}$) and $|V_{CC}| + |V_{EE}| \leq 60V$
Differential Input Voltage 60V
Output Current Internally Limited
Power Dissipation (Note 6) 62.5W
ESD Susceptability (Note 7) 3000V
Junction Temperature (Note 8) 150˚C
Thermal Resistance
- Non-Isolated T-Package $\theta_{JC}$ 1˚C/W
Soldering Information
- T Package 260˚C
Storage Temperature -40˚C to +150˚C

Operating Ratings (Notes 4, 5)

Temperature Range $T_{MIN} \leq T_A \leq T_{MAX}$ -20˚C ≤ $T_A$ ≤ +85˚C
Supply Voltage $|V_{CC}| + |V_{EE}|$ (Note 1) 20V to 60V

Electrical Characteristics (Notes 4, 5)
The following specifications apply for $V_{CC} = +30V$, $V_{EE} = -30V$, $I_{MUTE} = -0.5 mA$ with $R_L = 8 Ohm$ unless otherwise specified. Limits apply for $T_A > 25˚C$.

<table>
<thead>
<tr>
<th>Symbol</th>
<th>Parameter</th>
<th>Conditions</th>
<th>LM4766 Units (Limits)</th>
</tr>
</thead>
<tbody>
<tr>
<td>$</td>
<td>V_{CC}</td>
<td>+</td>
<td>V_{EE}</td>
</tr>
<tr>
<td>$P_{O}$ (Note 3)</td>
<td>Output Power (Continuous Average)</td>
<td>THD + N = 0.1% (max), $f = 1 kHz, f = 20 kHz$</td>
<td>40</td>
</tr>
<tr>
<td>THD + N</td>
<td>Total Harmonic Distortion Plus Noise</td>
<td>30 W/ch, $R_L = 8 Ohm$, $20 Hz \leq f \leq 20 kHz$</td>
<td>0.06</td>
</tr>
<tr>
<td>$X_{chan}$</td>
<td>Channel Separation</td>
<td>$f = 1 kHz, V_{O} = 10.9 Vrms$</td>
<td>60</td>
</tr>
<tr>
<td>$S_{R}$ (Note 3)</td>
<td>Slew Rate</td>
<td>$V_{IN} = 1.2 Vrms, t_{rise} = 2 ns$</td>
<td>9</td>
</tr>
<tr>
<td>$I_{Q_{MIN}}$ (Note 2)</td>
<td>Total Quiescent Power Supply Current</td>
<td>Both Amplifiers $V_{CM} = 0V$, $V_{O} = 0V, I_{Q} = 0 mA$</td>
<td>48</td>
</tr>
<tr>
<td>$V_{CC}$ (Note 2)</td>
<td>Input Offset Voltage</td>
<td>$V_{CM} = 0V, I_{O} = 0 mA$</td>
<td>1</td>
</tr>
<tr>
<td>$I_{O}$</td>
<td>Input Bias Current</td>
<td>$V_{CM} = 0V, I_{O} = 0 mA$</td>
<td>0.2</td>
</tr>
<tr>
<td>$I_{OS}$</td>
<td>Input Offset Current</td>
<td>$V_{CM} = 0V, I_{O} = 0 mA$</td>
<td>0.01</td>
</tr>
<tr>
<td>$I_{OL}$</td>
<td>Output Current Limit $</td>
<td>V_{CC}</td>
<td>+</td>
</tr>
<tr>
<td>$V_{CC}$ (Note 2)</td>
<td>Output Dropout Voltage (Note 12)</td>
<td>$</td>
<td>V_{CC}–V_{O}</td>
</tr>
<tr>
<td>PSRR (Note 2)</td>
<td>Power Supply Rejection Ratio</td>
<td>$V_{CC} = 30V$ to $10V, V_{EE} = -30V$, $V_{CM} = 0V, I_{O} = 0 mA$</td>
<td>125</td>
</tr>
<tr>
<td>CMRR (Note 2)</td>
<td>Common Mode Rejection Ratio</td>
<td>$V_{CC} = 30V$ to $10V, V_{EE} = -30V$ to $-10V$, $V_{CM} = 0V, I_{O} = 0 mA$</td>
<td>110</td>
</tr>
<tr>
<td>$P_{VCC}$ (Note 2)</td>
<td>Open Loop Voltage Gain</td>
<td>$R_L = 2 K\Omega, V_{O} = 40V$</td>
<td>115</td>
</tr>
<tr>
<td>GBWP</td>
<td>Gain Bandwidth Product</td>
<td>$f_{O} = 100 kHz, V_{IN} = 50 mVrms$</td>
<td>8</td>
</tr>
<tr>
<td>$E_{IN}$ (Note 3)</td>
<td>Input Noise</td>
<td>IHF—A Weighting Filter</td>
<td>2.0</td>
</tr>
</tbody>
</table>

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### Electrical Characteristics (Notes 4, 5) (Continued)

The following specifications apply for $V_{CC} = +30V$, $V_{EE} = −30V$, $I_{MUTE} = −0.5 mA$ with $R_L = 8\Omega$ unless otherwise specified. Limits apply for $T_A = 25^\circ C$.

<table>
<thead>
<tr>
<th>Symbol</th>
<th>Parameter</th>
<th>Conditions</th>
<th>LM766</th>
<th>Units (Limits)</th>
</tr>
</thead>
<tbody>
<tr>
<td>SNR</td>
<td>Signal-to-Noise Ratio</td>
<td>$P_O = 1W$, $A — Weighted$, Measured at 1 kHz, $R_S = 25\Omega$</td>
<td>98</td>
<td>dB</td>
</tr>
<tr>
<td></td>
<td></td>
<td>$P_O = 25W$, $A — Weighted$, Measured at 1 kHz, $R_S = 25\Omega$</td>
<td>112</td>
<td>dB</td>
</tr>
<tr>
<td>$A_{MM}$</td>
<td>Mute Attenuation</td>
<td>Pin 6,11 at 2.5V</td>
<td>115</td>
<td>80 dB (min)</td>
</tr>
</tbody>
</table>

**Note 1:** Operation is guaranteed up to 60V, however, distortion may be introduced from SPIKE Protection Circuitry if proper thermal considerations are not taken into account. Refer to the Application Information section for a complete explanation.

**Note 2:** DC Electrical Test; Refer to Test Circuit #1.

**Note 3:** AC Electrical Test; Refer to Test Circuit #2.

**Note 4:** All voltages are measured with respect to the GND pins (5, 10), unless otherwise specified.

**Note 5:** Absolute Maximum Ratings indicate limits beyond which damage to the device may occur. Operating Ratings indicate conditions for which the device is functional, but do not guarantee specific performance limits. Electrical Characteristics state DC and AC electrical specifications under particular test conditions which guarantee specific performance limits. This assumes that the device is within the Operating Ratings. Specifications are not guaranteed for parameters where no limit is given, however, the typical value is a good indication of device performance.

**Note 6:** For operating at case temperatures above 25$^\circ$C, the device must be derated based on a 150$^\circ$C maximum junction temperature and a thermal resistance of $\theta_{JC} = 1^\circ$C/W (junction to case) for the T package. Refer to the section Determining the Correct Heat Sink in the Application Information section.

**Note 7:** Human body model, 100 pF discharged through a 1.5 k$\Omega$ resistor.

**Note 8:** The operating junction temperature maximum is 150$^\circ$C, however, the instantaneous Safe Operating Area temperature is 250$^\circ$C.

**Note 9:** Typicals are measured at 25$^\circ$C and represent the parametric norm.

**Note 10:** Limits are guarantees that all parts are tested in production to meet the stated values.

**Note 11:** $V_{EE}$ must have at least −9V at its pin with reference to ground in order for the under-voltage protection circuitry to be disabled. In addition, the voltage differential between $V_{CC}$ and $V_{EE}$ must be greater than 14V.

**Note 12:** The output dropout voltage, $V_{OD}$, is the supply voltage minus the clipping voltage. Refer to the Clipping Voltage vs. Supply Voltage graph in the Typical Performance Characteristics section.

#### Test Circuit #1 (Note 2) (DC Electrical Test Circuit)

[Diagram of Test Circuit #1]
Test Circuit #2  (Note 3) (AC Electrical Test Circuit)

Bridged Amplifier Application Circuit

FIGURE 2. Bridged Amplifier Application Circuit
Single Supply Application Circuit

Note: *Optional components dependent upon specific design requirements.

Auxiliary Amplifier Application Circuit
Equivalent Schematic (excluding active protection circuitry)

LM4766 (One Channel Only)
### External Components Description

<table>
<thead>
<tr>
<th>Components</th>
<th>Functional Description</th>
</tr>
</thead>
<tbody>
<tr>
<td>1 ( R_b )</td>
<td>Prevents currents from entering the amplifier’s non-inverting input which may be passed through to the load upon power down of the system due to the low input impedance of the circuitry when the undervoltage circuitry is off. This phenomenon occurs when the supply voltages are below 1.5V.</td>
</tr>
<tr>
<td>2 ( R_i )</td>
<td>Inverting input resistance to provide AC gain in conjunction with ( R_f ).</td>
</tr>
<tr>
<td>3 ( R_f )</td>
<td>Feedback resistance to provide AC gain in conjunction with ( R_i ).</td>
</tr>
</tbody>
</table>
| 4 \( C_i \)  
(Note 13) | Feedback capacitor which ensures unity gain at DC. Also creates a highpass filter with \( R_i \) at \( f_C = 1/(2\pi R_i C_i) \). |
| 5 \( C_m \) | Provides power supply filtering and bypassing. Refer to the Supply Bypassing application section for proper placement and selection of bypass capacitors. |
| 6 \( R_v \)  
(Note 13) | Acts as a volume control by setting the input voltage level. |
| 7 \( R_{in} \)  
(Note 13) | Sets the amplifier’s input terminals DC bias point when \( C_{in} \) is present in the circuit. Also works with \( C_{in} \) to create a highpass filter at \( f_C = 1/(2\pi R_{in} C_{in}) \). Refer to Figure 4. |
| 8 \( C_{in} \)  
(Note 13) | Input capacitor which blocks the input signal’s DC offsets from being passed onto the amplifier’s inputs. |
| 9 \( R_{out} \)  
(Note 13) | Works with \( C_{out} \) to stabilize the output stage by creating a pole that reduces high frequency instabilities. |
| 10 \( C_{out} \)  
(Note 13) | Works with \( R_{out} \) to stabilize the output stage by creating a pole that reduces high frequency instabilities. The pole is set at \( f_C = 1/(2\pi R_{out} C_{out}) \). Refer to Figure 4. |
| 11 \( L \)  
(Note 13) | Provides high impedance at high frequencies so that \( R \) may decouple a highly capacitive load and reduce the Q of the series resonant circuit. Also provides a low impedance at low frequencies to short out \( R \) and pass audio signals to the load. Refer to Figure 4. |
| 12 \( R \)  
(Note 13) | Provides DC voltage biasing for the transistor Q1 in single supply operation. |
| 13 \( R_{in} \)  
(Note 13) | Limits the voltage difference between the amplifier’s inputs for single supply operation. Refer to the Clicks and Pops application section for a more detailed explanation of the function of \( R_{in} \). |
| 14 \( R_{bias} \)  
(Note 13) | Provides input bias current for single supply operation. Refer to the Clicks and Pops application section for a more detailed explanation of the function of \( R_{bias} \). |
| 15 \( R_{bias} \)  
(Note 13) | Establishes a fixed DC current for the transistor Q1 in single supply operation. This resistor stabilizes the half-supply point along with \( C_A \). |
| 16 \( R_{bias} \)  
(Note 13) | Mute resistance set up to allow 0.5 mA to be drawn from pin 6 or 11 to turn the muting function off. \( R_{bias} \) is calculated using: \( R_{bias} = (|V_{EE}| - 2.6V)/l \) where \( l \geq 0.5 \text{ mA} \). Refer to the Mute Attenuation vs Mute Current curves in the Typical Performance Characteristics section. |
| 17 \( C_A \)  
(Note 13) | Mute capacitance set up to create a large time constant for turn-on and turn-off muting. |
| 18 \( S_{1} \)  
(Note 13) | Mute switch that mutes the music going into the amplifier when opened. |

**Note 13:** Optional components dependent upon specific design requirements.

### Typical Performance Characteristics

**THD + N vs Frequency**

![THD + N vs Frequency](DS109205-S5)

**THD + N vs Frequency**

![THD + N vs Frequency](DS109205-S5)

**THD + N vs Output Power**

![THD + N vs Output Power](DS109205-S5)
Typical Performance Characteristics (Continued)

THD + N vs Output Power

Channel Separation vs Frequency

Clipping Voltage vs Supply Voltage

Output Power vs Supply Voltage

Power Dissipation vs Output Power
Typical Performance Characteristics (Continued)

Max Heatsink Thermal Resistance (°C/W)
at the Specified Ambient Temperature (°C)

<table>
<thead>
<tr>
<th>T_a (°C)</th>
<th>DS100928-75</th>
<th>DS100928-59</th>
<th>DS100928-60</th>
<th>DS100928-63</th>
<th>DS100928-64</th>
<th>DS100928-66</th>
<th>DS100928-87</th>
</tr>
</thead>
<tbody>
<tr>
<td>40</td>
<td>0.72</td>
<td>0.88</td>
<td>1.07</td>
<td>1.30</td>
<td>1.55</td>
<td>1.93</td>
<td>2.37</td>
</tr>
<tr>
<td>50</td>
<td>0.80</td>
<td>1.30</td>
<td>1.66</td>
<td>1.80</td>
<td>1.93</td>
<td>2.13</td>
<td>2.47</td>
</tr>
<tr>
<td>60</td>
<td>0.80</td>
<td>1.80</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.47</td>
</tr>
<tr>
<td>70</td>
<td>0.80</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.47</td>
</tr>
<tr>
<td>80</td>
<td>0.80</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.47</td>
</tr>
<tr>
<td>90</td>
<td>0.80</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.47</td>
</tr>
<tr>
<td>100</td>
<td>0.80</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.00</td>
<td>2.47</td>
</tr>
</tbody>
</table>

Note: The maximum heatsink thermal resistance values, θ_SA, in the table above were calculated using a θ_CS = 0.2°C/W due to thermal compound.
Application Information

MUTE MODE

The muting function of the LM4766 allows the user to mute the music going into the amplifier by drawing more than 0.5 mA out of each mute pin on the device. This is accomplished as shown in the Typical Application Circuit where the resistor RM is chosen with reference to your negative supply voltage and is used in conjunction with a switch. The switch when opened cuts off the current flow from pin 6 or 11 to VEE, thus placing the LM4766 into mute mode. Refer to the Mute Attenuation vs Mute Current curves in the Typical Performance Characteristics section for values of attenuation per current out of pins 6 or 11. The resistance RM is calculated by the following equation:

\[ R_M \leq \frac{|-V_{EE}| - 2.6V}{I_{pin6}} \]

where \( I_{pin6} = I_{pin11} \geq 0.5 \text{ mA} \).

Both pins 6 and 11 can be tied together so that only one resistor and capacitor are required for the mute function. The mute resistance must be chosen such that greater than 1 mA is pulled through the resistor R_M so that each amplifier is fully
Application Information (Continued)

DETERMINING MAXIMUM POWER DISSIPATION

Power dissipation within the integrated circuit package is a very important parameter requiring a thorough understanding if optimum power output is to be obtained. An incorrect maximum power dissipation calculation may result in inadequate heat sinking causing thermal shutdown and thus limiting the output power. Equation (1) exemplifies the theoretical maximum power dissipation point of each amplifier where \( V_{CC} \) is the total supply voltage.

\[
P_{D\text{MAX}} = V_{CC}^2 / 2 \pi R_L
\]

Thus by knowing the total supply voltage and rated output load, the maximum power dissipation point can be calculated. The package dissipation is twice the number which results from Equation (1) since there are two amplifiers in each LM4766. Refer to the graphs of Power Dissipation versus Output Power in the Typical Performance Characteristics section which show the actual full range of power dissipation not just the maximum theoretical point that results from Equation (1).

DETERMINING THE CORRECT HEAT SINK

The choice of a heat sink for a high-power audio amplifier is made entirely to keep the die temperature at a level such that the thermal protection circuitry does not operate under normal circumstances.

The thermal resistance from the die (junction) to the outside air (ambient) is a combination of three thermal resistances, \( \theta_{JC} \), \( \theta_{CS} \), and \( \theta_{SA} \). In addition, the thermal resistance, \( \theta_{JC} \) (junction to case), of the LM4766T is 1°C/W. Using Thermalloy Thermacote thermal compound, the thermal resistance, \( \theta_{CS} \) (case to sink), is about 0.2°C/W. Since convection heat flow (power dissipation) is analogous to current flow, thermal resistance is analogous to electrical resistance, and temperature drops are analogous to voltage drops, the power dissipation out of the LM4766 is equal to the following:

\[
P_{D\text{MAX}} = (T_{J\text{MAX}} - T_{AMB}) / \theta_{JA}
\]

Once the maximum package power dissipation has been calculated using Equation (1), the maximum thermal resistance, \( \theta_{JA} \) (heat sink to ambient) in °C/W for a heat sink can be calculated. This calculation is made using Equation (3) which is derived by solving for \( \theta_{JA} \) in Equation (2):

\[
\theta_{JA} = (T_{J\text{MAX}} - T_{AMB}) / P_{D\text{MAX}} - (\theta_{JC} + \theta_{CS} + \theta_{SA})
\]

Again it must be noted that the value of \( \theta_{JA} \) is dependent upon the system designer’s amplifier requirements. If the ambient temperature that the audio amplifier is to be working under is higher than 25°C, then the thermal resistance for the heat sink, given all other things are equal, will need to be smaller.

SUPPLY BYPASSING

The LM4766 has excellent power supply rejection and does not require a regulated supply. However, to improve system performance as well as eliminate possible oscillations, the LM4766 should have its supply leads bypassed with low-inductance capacitors having short leads that are located close to the package terminals. Inadequate power supply bypassing will manifest itself by a low frequency oscillation known as “motorboating” or by high frequency instabilities. These instabilities can be eliminated through multiple bypassing using a large tantalum or electrolytic capacitor (10 µF or larger) which is used to absorb low frequency variations and a small ceramic capacitor (0.1 µF) to prevent any high frequency feedback through the power supply lines.
Application Information (Continued)

If adequate bypassing is not provided, the current in the supply leads which is a rectified component of the load current may be fed back into internal circuitry. This signal causes distortion at high frequencies requiring that the supplies be bypassed at the package terminals with an electrolytic capacitor of 470 µF or more.

BRIDGED AMPLIFIER APPLICATION

The LM4766 has two operational amplifiers internally, allowing for a few different amplifier configurations. One of these configurations is referred to as “bridged mode” and involves driving the load differentially through the LM4766’s outputs. This configuration is shown in Figure 2. Bridged mode operation is different from the classical single-ended amplifier configuration where one side of its load is connected to ground.

A bridge amplifier design has a distinct advantage over the single-ended configuration, as it provides differential drive to the load, thus doubling output swing for a specified supply voltage. Consequently, theoretically four times the output power is possible as compared to a single-ended amplifier under the same conditions. This increase in attainable output power assumes that the amplifier is not current limited or clipped.

A direct consequence of the increased power delivered to the load by a bridge amplifier is an increase in internal power dissipation. For each operational amplifier in a bridge configuration, the internal power dissipation will increase by a factor of two over the single ended dissipation. Thus, for an audio power amplifier such as the LM4766, which has two operational amplifiers in one package, the package dissipation will increase by a factor of four. To calculate the LM4766’s maximum power dissipation point for a bridged load, multiply Equation (1) by a factor of four.

The value of $P_{D\text{max}}$ can be used to calculate the correct size heat sink for a bridged amplifier application. Since the internal dissipation for a given power supply and load is increased by using bridged-mode, the heatsink’s $R_h$ will have to decrease accordingly as shown by Equation (3). Refer to the section, Determining the Correct Heat Sink, for a more detailed discussion of proper heat sinking for a given application.

SINGLE-SUPPLY AMPLIFIER APPLICATION

The typical application of the LM4766 is a single supply amplifier. As shown in Figure 3, the resistors labeled $R_{BI}$ help bias up the LM4766 off the half-supply node at the emitter of the 2N3904. But due to the input and output coupling capacitors in the circuit, along with the negative feedback, there are two different values of $R_{BI}$, namely 10 kΩ and 200 kΩ. These resistors bring up the inputs at the same rate resulting in a popless turn-on. Adjusting these resistors values slightly may reduce pops resulting from power supplies that ramp extremely quick or exhibit overshoot during system turn-on.

CLICKS AND POPS

In the typical application of the LM4766 as a single-supply audio power amplifier, the IC exhibits excellent “click” and “pop” performance when utilizing the mute and standby modes. In addition, the device employs Under-Voltage Protection, which eliminates unwanted power-up and power-down transients. The basis for these functions are a stable and constant half-supply potential. In a split-supply application, ground is the stable half-supply potential. But in a single-supply application, the half-supply needs to charge up just like the supply rail, $V_{CC}$. This makes the task of attaining a clickless and popless turn-on more challenging. Any uneven charging of the amplifier inputs will result in output clicks and pops due to the differential input topology of the LM4766.

To achieve a transient free power-up and power-down, the voltage seen at the input terminals should be ideally the same. Such a signal will be common-mode in nature, and will be rejected by the LM4766. In Figure 3, the resistor $R_{BS}$ serves to keep the inputs at the same potential by limiting the voltage difference possible between the two nodes. This should significantly reduce any type of turn-on pop, due to an uneven charging of the amplifier inputs. This charging is based on a specific application loading and thus, the system designer may need to adjust these values for optimal performance.

As shown in Figure 3, the resistors labeled $R_{BS}$ help bias up the LM4766 off the half-supply node at the emitter of the 2N3904. But due to the input and output coupling capacitors in the circuit, along with the negative feedback, there are two different values of $R_{BS}$, namely 10 kΩ and 200 kΩ. These resistors bring up the inputs at the same rate resulting in a popless turn-on. Adjusting these resistors values slightly may reduce pops resulting from power supplies that ramp extremely quick or exhibit overshoot during system turn-on.

AUDIO POWER AMPLIFIER DESIGN

Design a 30W/8Ω Audio Amplifier

Given:
- Power Output: 30 W rms
- Load Impedance: 8 Ω
- Input Level: 1 Vrms (max)
- Input Impedance: 47 kΩ
- Bandwidth: 20 Hz–20 kHz
- Output Voltage: ±0.25 dB

A designer must first determine the power supply requirements in terms of both voltage and current needed to obtain the specified output power. $V_{\text{Opeak}}$ can be determined from Equation (4) and $I_{\text{Ppeak}}$ from Equation (5).

$$V_{\text{Opeak}} = \sqrt{2P_{\text{O}}R_L}$$  \hspace{1cm} (4)

$$I_{\text{Ppeak}} = \frac{\sqrt{2P_{\text{O}}}}{R_L}$$  \hspace{1cm} (5)

To determine the maximum supply voltage the following conditions must be considered. Add the dropout voltage to the peak output swing $V_{\text{Opeak}}$, to get the supply rail at a current of $I_{\text{Ppeak}}$. The regulation of the supply determines the unloaded voltage which is usually about 15% higher. The supply voltage will also rise 10% during high line conditions. Therefore the maximum supply voltage is obtained from the following equation.

$$V_{\text{D}} = \pm (V_{\text{Opeak}} + V_{\text{OD}}) (1 + \text{regulation})$$  \hspace{1cm} (1.1)

For 30W of output power into an 8Ω load, the required $V_{\text{Opeak}}$ is 21.91V. A minimum supply rail of 25.4V results from adding $V_{\text{Opeak}}$ and $V_{\text{OD}}$. With regulation, the maximum supplies are ±32V and the required $I_{\text{Ppeak}}$ is 2.74A from Equation (5). It should be noted that for a dual 30W amplifier into an 8Ω load the $I_{\text{Ppeak}}$ drawn from the supplies is twice 2.74 A or 5.48 A. At this point it is a good idea to check the Power Output vs Supply Voltage to ensure that the required output power is obtainable from the device while maintaining low THD+N. In addition, the designer should
Application Information (Continued)

Verify that with the required power supply voltage and load impedance, that the required heatsink value $\theta_{SA}$ is feasible given system cost and size constraints. Once the heatsink issues have been addressed, the required gain can be determined from Equation (6).

$$AV \geq \frac{(P_{OL})}{(V_{IN})} = \frac{V_{ORMS}}{V_{INRMS}} \quad (6)$$

From Equation (6), the minimum $AV$ is: $AV \geq 15.5$.

By selecting a gain of 21, and with a feedback resistor, $R_f = 20 \, k\Omega$, the value of $R_i$ follows from Equation (7).

$$R_i = R_f \times (AV - 1) \quad (7)$$

Thus with $R_i = 1 \, k\Omega$ a non-inverting gain of 21 will result. Since the desired input impedance was 47 k$\Omega$, a value of 47 k$\Omega$ was selected for $R_{INP}$. The final design step is to address the bandwidth requirements which must be stated as a pair of −3 dB frequency points. Five times away from a −3 dB point is 0.17 dB down from passband response which is better than the required ±0.25 dB specified. This fact results in a low and high frequency pole of 4 Hz and 100 kHz respectively. As stated in the External Components section, $R_i$ in conjunction with $C_i$ create a high-pass filter.

$$C_i \geq \frac{1}{(2\pi \times 1 \, k\Omega \times 4 \, Hz)} = 39.8 \, \mu F; \quad \text{use 39} \, \mu F.$$

The high frequency pole is determined by the product of the desired high frequency pole, $f_H$, and the gain, $AV$. With a $AV = 21$ and $f_H = 100$ kHz, the resulting GBWP is 2.1 MHz, which is less than the guaranteed minimum GBWP of the LM4766 of 8 MHz. This will ensure that the high frequency response of the amplifier will be no worse than 0.17 dB down at 20 kHz which is well within the bandwidth requirements of the design.
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